# 8.6 Stepped-Impedance Low-Pass Filters

**Reading Assignment:** *pp. 412-416*

Another distributed element realization of a lumped element low-pass filter designs is the **stepped-impedance** low-pass filter.

These filters are also know as **"hi-Z, low-Z"** filters, and we're about to find out why!

HO: STEPPED-IMPEDANCE LOW-PASS FILTERS

**Q:** *Are there* ***other*** *methods for building microwave filters?*

**A:** There are a **bundle** of them!

**All** distributed elements (e.g., transmission lines, coupled lines, resonators, stubs) exhibit **some** frequency dependency. If we are clever, we can construct these structures in a way that their frequency dependency (i.e., $S_{21}(\omega)$) conforms to a desirable function of $\omega$.

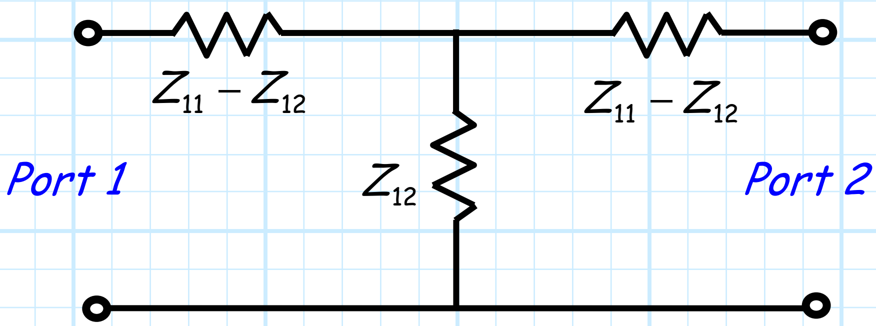
Other examples of filter realizations—ones applicable to **band-pass** filters—are discussed in sections **8.7** and **8.8** of your book.

# Stepped-Impedance Low-Pass Filters

Say we know the impedance matrix of a **symmetric** two-port device:

$$\mathcal{Z} = \begin{bmatrix} Z_{11} & Z_{21} \\ Z_{21} & Z_{11} \end{bmatrix}$$

**Regardless** of the construction of this two port device, we can **model** it as a simple "T-circuit", consisting of three impedances:

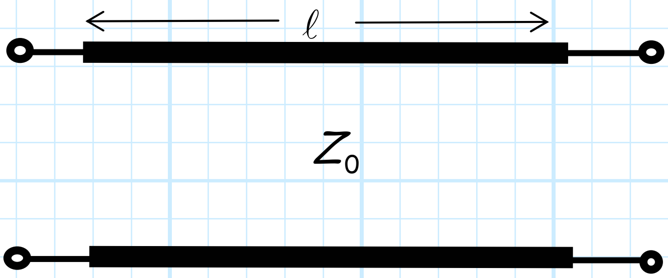



In other words, if the two **series impedances** have an impedance value equal to $Z_{11} - Z_{21}$, and the **shunt impedance** has a value equal to $Z_{21}$, the impedance matrix of this "T-circuit" is:

$$\mathcal{Z} = \begin{bmatrix} Z_{11} & Z_{21} \\ Z_{21} & Z_{11} \end{bmatrix}$$

Thus, **any** symmetric two-port network can be modeled by this "T-circuit"!

For example, consider a length $\ell$ of **transmission line** (a symmetric two-port network!):




Recall (or determine for yourself!) that the **impedance parameters** of this two port network are:

$$Z_{11} = Z_{22} = -jZ_0 \cot \beta\ell$$

$$Z_{12} = Z_{21} = -jZ_0 \csc \beta\ell$$

With a little **trigonometry**, ICBST :


$$Z_{11} - Z_{12} = j\, Z_0 \tan\left(\frac{\beta\ell}{2}\right)$$

Furthermore, if $\beta\ell$ is **small**:

$$\sin \beta\ell \approx \beta\ell \qquad \cos \beta\ell \approx 1 \qquad \tan \beta\ell \approx \beta\ell$$

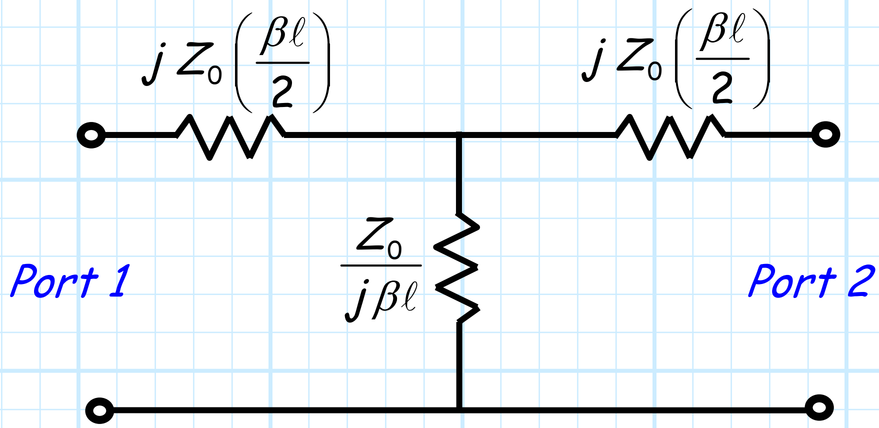
where $\beta\ell$ is expressed in **radians**. Thus,

$$Z_{11} - Z_{12} \approx j\, Z_0 \left(\frac{\beta\ell}{2}\right)$$

and also:

$$Z_{12} = Z_{21} = -jZ_0 \csc \beta\ell \approx \frac{Z_0}{j\beta\ell}$$

Thus, an **electrically short** ($\beta\ell \ll 1$) transmission line can be **approximately modeled** with a "T-circuit" as:



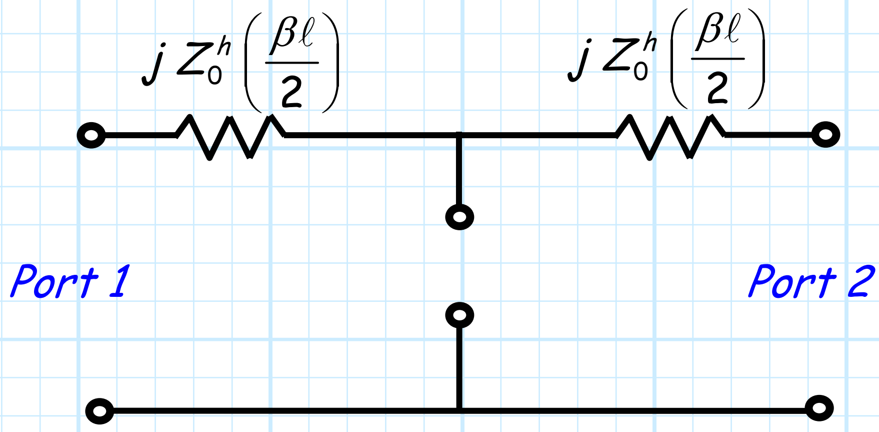

Now, consider also the case where the **characteristic impedance** of the transmission line is **relatively large**. We'll **denote** this large characteristic impedance as $Z_0^h$.

Note the **shunt** impedance, value $Z_0^h / j\beta\ell$. Since the **numerator** ($Z_0^h$) is relatively **large**, and the **denominator** ($j\beta\ell$) is **small**, the impedance shunt device is **very large**.

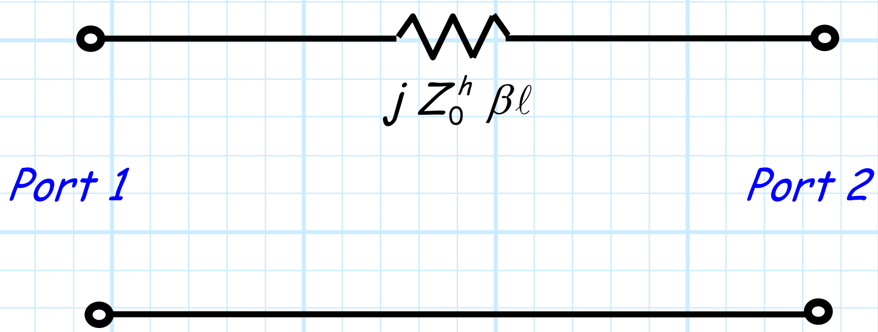
So large, in fact, that we can approximate it as an **open circuit**!

$$\frac{Z_0^h}{j\beta\ell} \approx \infty \qquad \text{for } \beta\ell \ll 1 \text{ and } Z_0^h \gg Z_0$$

So now we have a further **simplification** of our **model**:




The remaining impedances are now in **series**, so the circuit can be further simplified to:




*The equivalent circuit for transmission line with short electrical length ($\beta\ell \ll 1$) and large characteristic impedance $Z_0^h$ ($Z_0^h \gg Z_0$).*

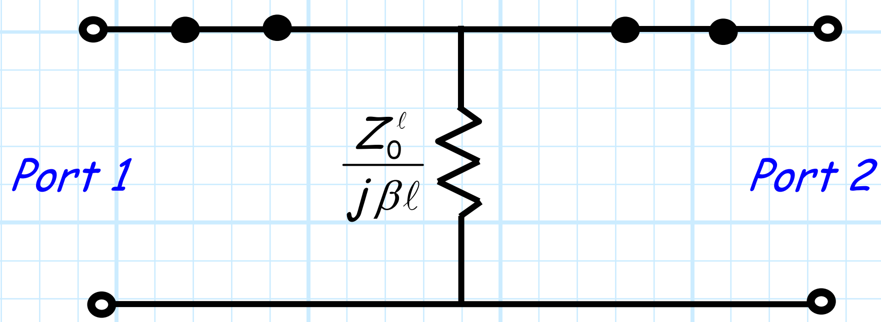
Now, consider the case where the **characteristic impedance** of the transmission line has a relatively **low value**, denoted as $Z_0^\ell$, where $Z_0^\ell \ll Z_0$.

Note the **series** impedance, values $j\,Z_0^\ell\,(\beta\ell/2)$. Since both $Z_0^\ell$ and $\beta\ell$ are **small**, the product of the two is **very small**.

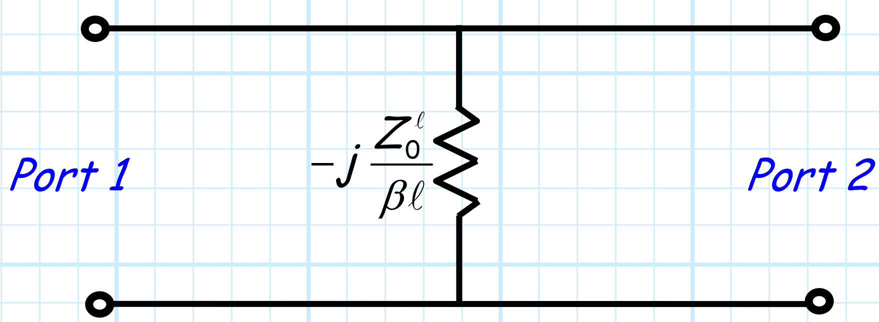
So small, in fact, that we can approximate it as a **short circuit**!

$$jZ_0^{\ell}\left(\frac{\beta\ell}{2}\right) \approx 0 \qquad \text{for } \beta\ell \ll 1 \text{ and } Z_0^{\ell} \ll Z_0$$

So now we have **another simplification** of our model:




Which **of course** further simplifies to:




*The equivalent circuit for transmission line with short electrical length ($\beta\ell \ll 1$) and small characteristic impedance $Z_0^{\ell}$ ($Z_0^{\ell} \ll Z_0$).*

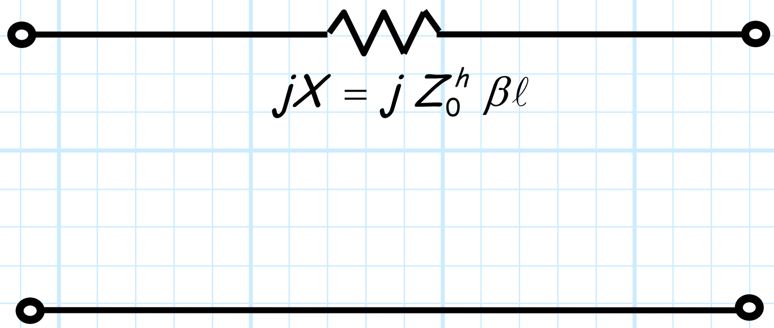
**Q:** *But, **what** does all this have to do with constructing a **low-pass filter**?*

**A:** **Plenty!** Recall that a lossless low-pass filter constructed with **lumped** elements consists of a "circuit ladder" of **series inductors** and **shunt capacitors**!

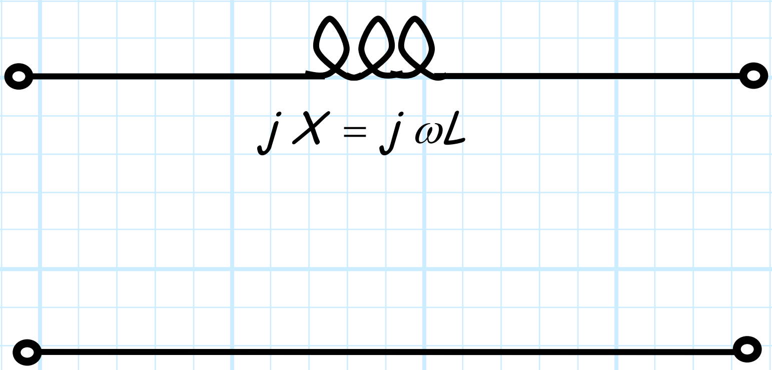
**Q:** *So?*

**A:** Look at the two **equivalent circuits** for an electrically short transmission line. The one with **large** characteristic impedance $Z_0^h$ has the form of a **series inductor**, and the one with **small** characteristic impedance $Z_0^\ell$ has the form of a **shunt capacitor**!

I.E.:




and:




are identical **if**:

$$j\,Z_0^h\,\beta\ell = j\omega L \quad \Rightarrow \quad Z_0^h\,\beta\ell = \omega L$$

Thus, the "**series inductance**" of our **transmission line** length is:

$$L = \frac{Z_0^h \, \beta\ell}{\omega}$$

**Q:** *Yikes! Our inductance appears to be a function of **frequency** $\omega$. I **assume** we simply **set** this value to **cutoff frequency** $\omega_c$, just like we did for Richard's transformation?*

**A:** **Nope!** We can **simplify** the result a bit more. Recall that $\beta = \omega / v_p$, so that:

$$L = \frac{Z_0^h \, \beta\ell}{\omega} = \frac{Z_0^h \, \ell}{v_p}$$

In other words, the **series impedance** resulting from our short transmission line is:

$$Z = j\omega \left( \frac{Z_0^h \, \ell}{v_p} \right)$$

**Q:** ***Wow!** This realization seems to give us a result that **precisely** matches an inductor at **all** frequencies—**right**?*

**A:** **Not** quite! Recall this result was obtained from applying a few **approximations**—the result is **not** exact!

**Moreover**, one of these approximations was that the **electrical length** of the transmission line be **small**. This obviously **cannot** be true at **all** frequencies. As the signal frequency **increases**, so does the **electrical length**—our **approximate** solution will **no longer be valid**.

hus, this realization is accurate **only** for "**low** frequencies"—recall that was **likewise** true for **Richard's transformations**!

**Q:** *Low-frequencies? How **low** is **low**?*

**A:** Well, for our filter to provide a response that **accurately** follows the **lumped element** design, our approximation should be valid for frequencies **up to** (and including!) the **filter cutoff frequency** $\omega_c$.

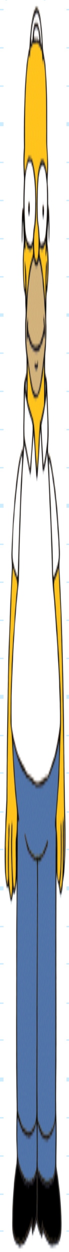
A general "**rule-of-thumb**" is that a **small electrical length** is defined as being **less than** $\pi/4$ radians. Thus, to maintain this small electrical length at frequency $\omega_c$, our realization **must** satisfy the relationship:

$$\beta_c \ell = \frac{\omega_c L}{Z_0^h} < \frac{\pi}{4}$$

Note that this criterion is **difficult** to satisfy if the **filter cutoff frequency** and/or the **inductance value** $L$ that we are trying to realize is **large**.

Our **only** recourse for these challenging conditions is to **increase** the value of **characteristic impedance** $Z_0^h$.

**Q:** *Is there some particular difficulty with increasing $Z_0^h$?*



**A: Could be!** There is always a **practical** limit to how large (or small) we can make the **characteristic impedance** of a transmission line.

For example, a **large** characteristic impedance implemented in **microstip/stripline** requires a **very narrow** conductor **width** ***W***. But manufacturing tolerances, power handling capability and/or line loss (line resistance $R$ increases as $W$ decreases) place a **lower bound** on how **narrow** we can make these conductors!

However, assuming that we **can** satisfy the above constraint, we can approximately "**realize**" a **lumped inductor** of inductance **value** ***L*** by selecting the correct **characteristic impedance** $Z_0^h$ and **line length** $\ell$ of our short transmission line:

$$L = \frac{Z_0^h \, \ell}{v_p}$$

**Q:** *For **Richard's Transformation**, we **first** set the stub length to a **fixed** value (i.e.,* $\ell = \lambda_c/8$*), and **then** determined the **specific characteristic impedance** necessary to realize a **specific inductor value** L. I **assume** we follow the same procedure here?*

**A: Nope!** When constructing stepped-impedance low-pass filters, we typically do the **opposite**!

**1) First**, we select the value of $Z_0^h$, making sure that the short electrical length inequality is **satisfied** for the **largest inductance value** $L$ in our lumped element filter:

$$Z_0^h > \frac{4\,\omega_c\,L}{\pi}$$

This characteristic impedance value is typically used to realize **all** inductor values $L$ in our low-pass filter, **regardless** of the actual value of inductance $L$.

**2)** Then, we determine the **specific lengths** $\ell_n$ of the transmission line required to realize **specific** filter **inductors values** $L_n$:

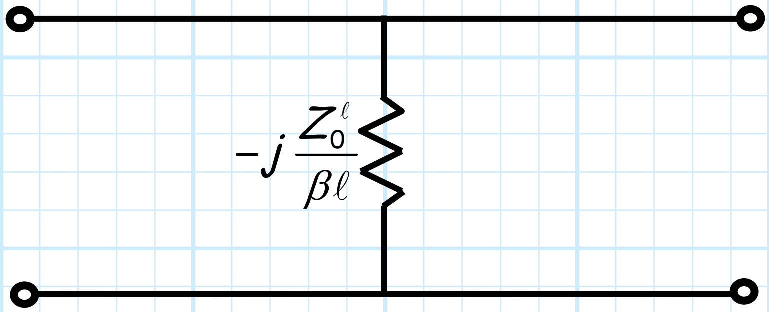
$$\ell_n = \left(\frac{v_p}{Z_0^h}\right) L_n$$

**Q:** *What about the **shunt capacitors**?*

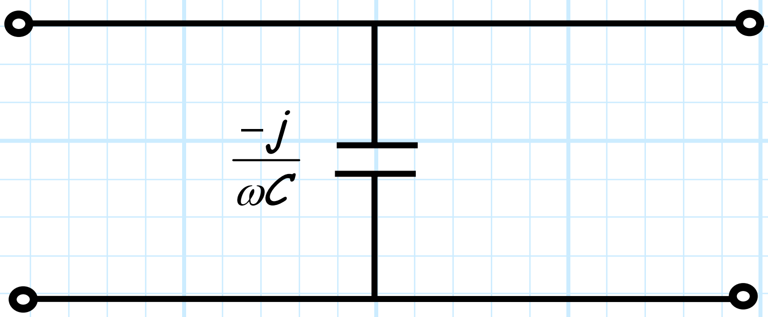
**A:** Almost forgot!

Recall the **low-impedance** transmission line provided a **shunt impedance** that matched a shunt capacitor:

I.E.:




and:




are identical if:

$$-j\,\frac{Z_0^\ell}{\beta\ell} = -j\,\frac{1}{\omega C} \quad \Rightarrow \quad \frac{\beta\ell}{Z_0^\ell} = \omega C$$

Thus, the "**shunt capacitance**" of our transmission line length is:

$$C = \frac{\beta\ell}{\omega\, Z_0^\ell}$$

But again using the fact that $\beta = \omega / v_p$ :

$$C = \frac{\ell}{v_p\, Z_0^\ell}$$

And thus the **shunt reactance** of our transmission line realization is:

$$Z = \frac{-j}{\omega}\left(\frac{v_p\, Z_0^{\ell}}{\ell}\right)$$

Although this again **appears** to provide **exactly** the same behavior as a **capacitor** (as a function of frequency), it is likewise accurate **only** for **low frequencies**, where $\beta\ell < \pi/4$.

Thus from our realization **equality**:

$$\frac{\beta\ell}{Z_0^{\ell}} = \omega C$$

We can conclude that for our approximations to be valid at all frequencies **up to** the filter **cutoff frequency**, the following inequality **must** be valid:

$$\beta_c \ell = \omega_c\, C\, Z_0^{\ell} < \frac{\pi}{4}$$

Note that for **difficult** design cases where $\omega_c$ and/or $C$ is **very large**, the line **characteristic impedance** $Z_0^{\ell}$ must be made **very small**.

**Q:** *I suppose there is **likewise** a problem with making $Z_0^{\ell}$ **very small**?*


**A:** Yes! In microstrip and stripline, making $Z_0^\ell$ **small** means making conductor width $W$ **very large**. In other words, it will take up **lots of space** on our substrate. For most applications the **surface area** of the substrate is both **limited** and precious, and thus there is generally a **practical limit** on how wide we can make width $W$ (i.e., how **low** we can make $Z_0^\ell$).

However, assuming that we **can** satisfy the above constraint, we can approximately **"realize"** a **lumped capacitor** of inductance value $C$ by selecting the correct **characteristic impedance** $Z_0^\ell$ and **line length** $\ell$ of our short transmission line:

$$C = \frac{\ell}{v_p \, Z_0^\ell}$$

The **design rules** for **shunt capacitor realization** are thus:

**1) First**, we select the value of $Z_0^\ell$, making sure that the short electrical length inequality is **satisfied** for the **largest** capacitance value $C$ in our lumped element filter:

$$Z_0^\ell < \frac{\pi}{4\,\omega_c\,C}$$

This characteristic impedance value is typically used to realize **all** capacitor values $C$ in our low-pass filter, **regardless** of the actual value of capacitance $C$.

**2)** Then, we determine the **specific lengths** $\ell_n$ of the transmission line required to realize **specific** filter capacitor values $C_n$:

$$\ell_n = \left(Z_0^h v_p\right) C_n$$

An **example** of a low-pass, stepped-impedance filter design is provided on page 414-416 of **your** book (but of course, **you** already knew that—**right**?).